# Control of a Direct Matrix Converter with Modulated Model Predictive Control

*Abstract*—This paper investigates the use of a model- predictive control strategy to control a direct matrix converter. The proposed control method combines the features of the classical Model Predictive Control and the Space Vector Modulation technique into a Modulated Model Predictive Control. This new solution maintains all the characteristics of Model Predictive Control (such as fast transient response ,multi-objective control using only one feedback loop, easy inclusion of non-linearities and constraints of the system, the flexibility to include other system requirements in the controller) adding the advantages of working at fixed switching frequency and improving the quality of the controlled waveforms. Simulation and experimental results employing the control method to a direct matrix converter are presented.

*Index Terms*—Matrix Converter, Model Predictive Control, Modulated Model Predictive Control.



Fig. 1. Schematic of a direct matrix converter system

## I. INTRODUCTION

A direct matrix converter(MC) is a AC/AC converter that is capable of converting varying amplitude, fixed frequency input to varying amplitude and frequency output without employing an intermediate DC-link capacitor. Nine bidirectional voltage-blocking current-conducting switches arranged in the form of a matrix as shown in Fig. 1 constitutes a MC making it possible for bidirectional power flow. In the recent years, MCs have reached a good level of technological maturity that allows their practical and industrial implementation in a variety of applications, such as industrial drives [1-2], power supplies [3], aerospace applications [4-7]. MC is often known as an all silicon converter as there are no bulky and heavy energy storage devices [8].

The first matrix converter modulation strategy was proposed by Alesina and Venturini [9]. Even though the initial strategy proposed was capable of producing sinusoidal input and output waveforms, the maximum voltage ratio it could achieve was only 0.5. Later several other modulation techniques which produce a higher voltage transfer ratio of 0.866 such as Optimum Venturini Modulation and Space Vector Modulation (SVM) were proposed later and SVM became the most widely used modulation method for MC [10]. Since then, SVM has been applied in many applications in conjunction with feedback control strategies in order to regulate specific control variables[11].

Model Predictive Control (MPC), introduced in the late seventies [12] considers a model of the system in order to predict its future behaviour over a time horizon. A cost function represents the desired behaviour of the system. MPC is an optimization problem where a sequence of future actuations is obtained by minimizing the cost function. It is also referred to as a receding horizon control, which means that at each instant the horizon is moved forward, the first
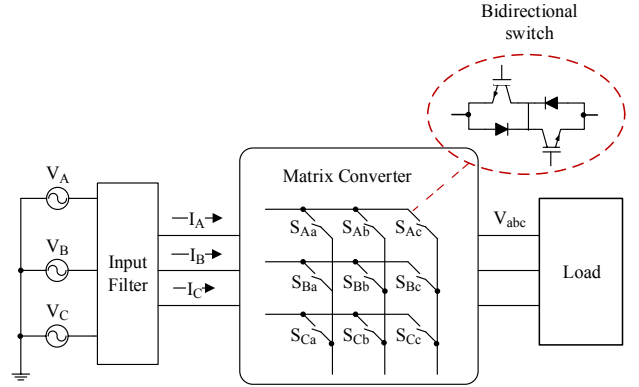
element of the sequence calculated at each step is applied at that instant and all the calculation is repeated every sample period [13]. Due to the high sampling rate used in the control of power converters, solving the optimization problem of MPC online is not practical. One approach is to use an explicit solution of MPC, solving the optimization problem offline. The resulting controller is a lookup table and can be implemented without big computational effort. Considering that power converters are systems with a finite number of states, given by the possible combinations of the state of the switching devices, the MPC optimization problem can be simplified and reduced to the prediction of the behaviour of the system for each possible state. Then, each prediction is evaluated using the cost function and the state that minimizes it, is selected. This approach has been successfully applied in recent years for the control of power converters and drives, like for current control and power control for three phase Voltage Sourse Inverters [13-14] and for current and torque control for induction motor and permanent magnet motor drives[15-17]. Even though control of currents, torque and flux are achieved, the switching frequency is variable and not fixed. MPC presents several advantages, such as fast dynamic response, easy inclusion of nonlinearities and constraints of the system, flexibility to include other system requirements in the controller, easy tuning of the control if the system model is known and the possibility of modifying and extending the methodology depending on specific applications.

One of the interesting features of MPC is that due to the absence of a modulator, the control chooses and applies one converter switching state for the entire sampling instant. This generates large ripples in the waveforms resulting in variable and high switching frequencies compared to other control methods. Various methods have been proposed in the literature to improve the applied vector sequence [18] or to

introduce a modulation scheme inside the MPC algorithm [19]. However these methods involve complicated expressions for the switching time patterns and are not flexible enough to include other system requirements in the cost function. This is overcome by modulated model predictive control (M2PC) which has been proposed for a cascaded H-bridge converter [20-22], active front-end rectifier [23], two level inverter [24], three phase rectifier [25], a neutral point clamp converter [26] and indirect matrix converter [27]. Inspired from this new approach, [28] elaborates the application of M2PC for a direct matrix converter and includes experimental results to validate the simulation results discussed in [29]. This paper includes a comparison of the performance of M2PC with conventional control methods such as MPC and Proportional-Integral (PI) controller.

## II. SYSTEM MODEL

In order to design the control system, an accurate model is required. The model description can be divided into matrix converter model and load model as presented in the following subsections.

### A. Matrix converter model

The voltages at the output of a matrix converter and input currents are calculated from the input voltages and output currents respectively and can be derived directly from Fig. 1. The voltages and currents are represented in terms of the switching functions related to each bidirectional switch in the matrix converter as shown in equations (1) and (2).

$$
\begin{bmatrix} v_a(t) \\ v_b(t) \\ v_c(t) \end{bmatrix} = \begin{bmatrix} S_{Aa}(t) & S_{Ba}(t) & S_{Ca}(t) \\ S_{Ab}(t) & S_{Bb}(t) & S_{Cb}(t) \\ S_{Ac}(t) & S_{Bc}(t) & S_{Cc}(t) \end{bmatrix} \cdot \begin{bmatrix} v_A(t) \\ v_B(t) \\ v_C(t) \end{bmatrix} \tag{1}
$$

$$
\begin{bmatrix} i_A(t) \\ i_B(t) \\ i_C(t) \end{bmatrix} = \begin{bmatrix} S_{Aa}(t) & S_{Ba}(t) & S_{Ca}(t) \\ S_{Ab}(t) & S_{Bb}(t) & S_{Cb}(t) \\ S_{Ac}(t) & S_{Bc}(t) & S_{Cc}(t) \end{bmatrix}^T \cdot \begin{bmatrix} i_a(t) \\ i_b(t) \\ i_c(t) \end{bmatrix} \tag{2}
$$

where $i_a(t), i_b(t)$ and $i_c(t)$ are the output currents, $i_A(t), i_B(t)$ and $i_C(t)$ the input currents, $v_a(t), v_b(t)$ and $v_c(t)$ the output voltages and $v_A(t), v_B(t)$ and $v_C(t)$ the source voltages and $S_{ij}(t)$ is the switching function for i= A,B and C and j= a,b and c.

### B. Load model

To determine the load current in the next sampling interval, a mathematical model of the load is required. Matrix converters are usually connected to an inductive load and hence this paper considers the model of a RL load to demonstrate M2PC. If M2PC needs to be implemented for MC feeding other loads such as an induction machine or a capacitive load, the load model needs to be derived appropriately. It is vital to the performance of the controller that the load model is accurate.

The continuous time model of a resistive-inductive load is given by equation (3).

$$
L\frac{di_o(t)}{dt} = v_o(t) - R\,i_o(t) \tag{3}
$$

where R and L are the load resistance and inductance respectively, $i_o(t) = [i_a(t)\ i_b(t)\ i_c(t)]^T$ the load currents and $v_o(t) = [v_a(t)\ v_b(t)\ v_c(t)]^T$ the matrix converter output voltage.

Discretising equation (3), using forward Euler approximation, the discrete time model of the load can be obtained as shown in equation (4).

$$
I_o(k+1) = (1 - \frac{RT_s}{L})I_o(k) + \frac{T_s}{L}V_o(k) \tag{4}
$$

Equation (4) is then used to predict the load currents at the future sampling instants in order to formulate the cost functions.

## III. MODULATED MODEL PREDICTIVE CONTROL FOR DIRECT MATRIX CONVERTER

The M2PC strategy aims to combine the positive features of both SVM and MPC to obtain a model predictive control based algorithm with an intrinsic modulation scheme. A basic control block diagram of the proposed strategy for a direct matrix converter is given in Fig. 2.
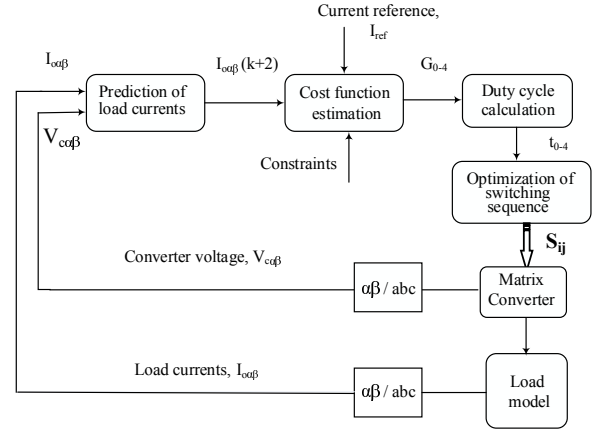


Fig. 2. Control block diagram for M2PC strategy

A reference current is imposed upon the system and the controller is designed using the system model so that the load current tracks the reference. The measured currents are then used to predict the value of current at (k+1). The reference and predicted currents are then used to calculate the cost function which in turn is used to derive the duty cycles for the selected voltage vectors. Unlike 2-level inverters with two active and three zero vectors, matrix converter usually makes use of four active and three zero vectors to obtain sinusoidal waveforms. Active vectors are those vectors that produce a non zero voltage. Zero vectors as the name suggests does not produce any voltage.

The M2PC utilizes the SVM vector sequence and calculates the duty cycles for each voltage vector based on the minimization of the cost function. Fixed switching frequency is

ensured in this case as the sequence of the vectors chosen by the control will be applied within one sampling interval. The difference between a classical MPC and the M2PC is in the application time of the vectors. Unlike MPC where one vector is applied for the whole sampling interval, in the M2PC at each sampling interval; four active and three zero vectors are selected by the cost function minimization algorithm and are applied for their respective duty cycles. The active and zero vectors are then arranged in a symmetrical manner as shown in Fig. 3; to achieve minimum switching losses and reduce harmonics. The switching pattern is similar to that used in a standard SVM scheme. $t_{01}, t_{02}$ and $t_{03}$ are the application times for the three zero vectors and $t_1, t_2, t_3$ and $t_4$ for the four active vectors.
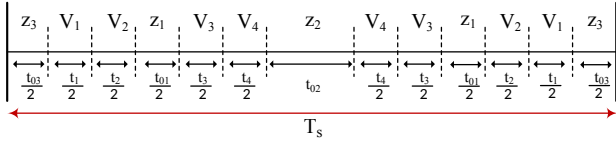


Fig. 3. Symmetrical switching pattern for a direct matrix converter

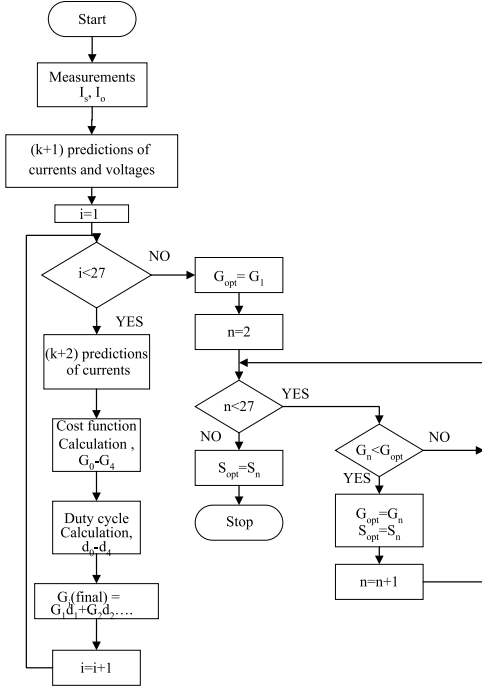Fig. 4 shows the flowchart of M2PC algorithm incorporating delay compensation for the computation.



Fig. 4. Flowchart showing the M2PC algorithm

### A. Prediction of Control Variables and Cost function calculation

Similar to the MPC, the switching states are calculated based on a cost function minimization. The cost function can include different performance factors according to the control variables and to the constraints required. More than one variable can be controlled with the same control loop, providing

a multi-objective control approach and avoiding nested loops. In this paper, the M2PC algorithm is provisionally applied to a direct matrix converter feeding a RL load to demonstrate current control capability.

For an RL load, the prediction of load current makes use of the current measurement at the present instant or instant 'k' and the load parameters as shown in (4). For MPC, the prediction of load current is carried out once using the optimal switching state from the previous instant. Since the M2PC incorporates a modulation scheme, more than one active vector will be applied during one sampling interval. For a direct matrix converter, out of the 27 switching states, the six rotating vectors are not considered for modulation resulting in 21 switching states to choose from. As in a standard SVM strategy [10] it is assumed that a minimum of four active vectors is required to get sinusoidal waveforms for a matrix converter. Hence the M2PC strategy will also consider four active vectors and three zero vectors to apply during one sampling interval. The predictions for four active vectors and zero vectors are done as if they were applied for the whole sampling interval. For example, for one sequence containing four active and three zero vectors, the predictions of load current are calculated as shown in equations (5) and (6). The predicted value of load current for the three zero vectors will be the same and hence it is only required to calculate once.

For active vectors :

$$I_o^i(k+1) = (1 - \frac{RT_s}{L})I_o^i(k) + \frac{T_s}{L}V_o^i(k) \qquad (5)$$

for i=1,2,..4.

For zero vectors:

$$I_o(k+1) = (1 - \frac{RT_s}{L})I_o(k) \qquad (6)$$

Once the currents at (k+1) instant are predicted, (k+2) predictions can be made by substituting $I_o(k)$ with $I_o(k+1)$ in equations (5) and (6).

Just as in MPC, the switching states are selected based on a cost function minimization. The cost function can include different performance factors according to the control variables and constraints required. More than one variable can be controlled with the same control loop, providing a multi-objective control approach and avoiding nested loops.

The cost function for load current control is essentially the error between the current demand and predicted current at (k+2) instant if the computation delay is compensated. This results in five cost functions $G_0, G_1, G_2, G_3$ and $G_4$ for each active and zero vectors. The set of quadratic cost functions can be calculated using the pre-calculated predicted currents in equation (5) as shown in (7).

$$G_i = (I_{oref}(k+2) - I_o^i(k+2))^2 \qquad (7)$$

for i=0,1,...4.

where $I_{oref}(k+2)$ is the current demand at (k+1) instant.

The final cost function used for the minimization algorithm constitutes the cost functions for the active and zero vectors and is expressed as shown in equation (8). The minimization

algorithm is run for 18 combinations of active and zero vector sequences.

$$G(final) = G_1 d_1 + G_2 d_2 + G_3 d_3 + G_4 d_4 + G_0 d_0 \quad (8)$$

where $d_0, d_1, d_2, d_3$ and $d_4$ are the duty cycles for the voltage vectors.

Once the cost functions for each of the active and zero vectors are calculated; the predictive control will choose the best sequence of vectors which produces the lowest error. These vectors are then applied within the sampling interval with their respective duty cycles. The duty cycles are calculated based on the cost functions values of the active and zero vectors.

The multi-objective control capability of the M2PC can be achieved by simply adding the control variables to the cost function for each vector and by specifying a weighting factor for each of them. In this manner, it is possible to also consider certain constraints for the optimal operation of the system. This is demonstrated in [30] by controlling the stator currents and input reactive power of an induction motor fed by a direct matrix converter without the use of nested loops.

*B. Calculation of Duty Cycles*

The application times for each of the vectors are calculated from the cost functions computed for each the switching state. This method is based on the assumption that per sampling interval, the system behavior is linear in nature. From this it is possible to derive the application times for each vector as a percentage of the total sampling time. The relation between the application times of the vectors and their corresponding cost functions can be written as follows.

$$t = \frac{k_1}{G} \quad (9)$$

where $k_1$ is the proportional constant and G is the cost function. Using the above equation for four active vectors and zero vector for a MC will result in a set of five equations, each dictating the application times for a particular vector in terms of the proportional constant. The condition that holds true for all the vectors applied is that the sum of the application times for all the vectors should be equal to the sampling time as shown in (10).

$$t_1 + t_2 + t_3 + t_4 + t_0 = T_s \quad (10)$$

where $t_1, t_2, t_3, t_4$ are the times for the four active vectors and $t_0$ is the time for three zero vectors. By substituting equation (9) in (10), the proportional constant can be obtained as shown in (11).

$$k_1 = \frac{G_0 G_1 G_2 G_3 G_4 T_s}{A} \quad (11)$$

where $A = (G_1 G_2 G_3 G_4 + G_0 G_2 G_3 G_4 + G_0 G_1 G_3 G_4 + G_0 G_1 G_2 G_4 + G_0 G_1 G_2 G_3)$.

The application times for the vectors can then be derived by substituting the value of the proportional constant. The resulting set of duty cycles is shown in equation (12).

$$t_1 = \frac{(G_0 G_2 G_3 G_4 T_s)}{A}$$
$$t_2 = \frac{(G_0 G_1 G_3 G_4 T_s)}{A}$$
$$t_3 = \frac{(G_0 G_1 G_2 G_4 T_s)}{A} \quad (12)$$
$$t_4 = \frac{(G_0 G_1 G_2 G_3 T_s)}{A}$$

Once the application times for active vectors are obtained, the time for zero vectors can be calculated from equation (10).

$$t_0 = T_s - (t_1 + t_2 + t_3 + t_4) \quad (13)$$

The duty cycles for each of the vector will be related to the error associated with that voltage vector. The direct relation of the duty cycles with the cost functions makes this method unique. The active and zero vectors are then applied for their respective duty cycles within one sampling interval.

The active and zero vectors are then arranged in a symmetrical manner as shown in Fig. 3; to achieve minimum switching losses and reduced harmonics. The switching pattern is similar to that used in a SVM scheme. $t_{01}, t_{02}$ and $t_{03}$ are the application times for the three zero vectors and $t_1, t_2, t_3$ and $t_4$ for the four active vectors in Fig. 3.

The switching frequency that can be attained using this method depends on the computational speed of the microprocessor being used. The matrix converter requires a significant computational overhead for this method since 27 switching states are available. The maximum controller update frequency obtained for M2PC within the laboratory when using a Texas Instruments C6713 DSP was 20kHz.

## IV. SIMULATION RESULTS

The M2PC is applied to a direct matrix converter feeding an RL load and simulations are done in Matlab Simulink environment to study its performance. A sampling time of $80\mu s$ is considered. The simulation also takes into account the four-step commutation in matrix converter and the measurement delays in the control platform. An LC input filter with a damping resistor is employed to mitigate the high frequency components of the input current of the matrix converter. A control block diagram showing the different steps involved in the load current control of a direct matrix converter using M2PC is shown in Fig. 5.
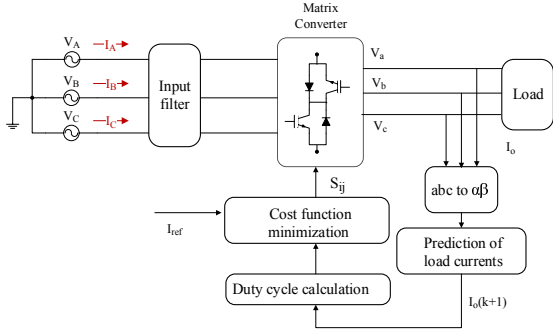
Fig. 5. Control block diagram of M2PC for a matrix converter

The system parameters for both the simulation and experimental tests are given in Table. I.

TABLE I
SYSTEM PARAMETERS

| Parameter | Value | Unit |
|---|---|---|
| Filter inductance | 0.7 | $mH$ |
| Filter capacitance (delta) | 8.3 | $\mu F$ |
| Damping resistor | 15 | $\Omega$ |
| Load resistance | 10 | $\Omega$ |
| Load inductance | 3.75 | $mH$ |
| Sampling time | 80 | $\mu s$ |

The load current of a matrix converter feeding an RL load is controlled using M2PC and the resulting waveforms are shown below. A load current reference of 5A at 30Hz is demanded from the system. Fig. 6 shows the controlled three phase load currents, MC line voltage at steady state and the Fast Fourier Transform (FFT) of the load current at steady state. It is worth noting the presence of harmonics in the range of switching frequency, 12.5kHz and its multiples. This is a result of fixed switching frequency operation. To analyse the quality of the controlled waveforms the Total Harmonic Distortion (THD) of Phase A load current is calculated and is approximately 6.3%.
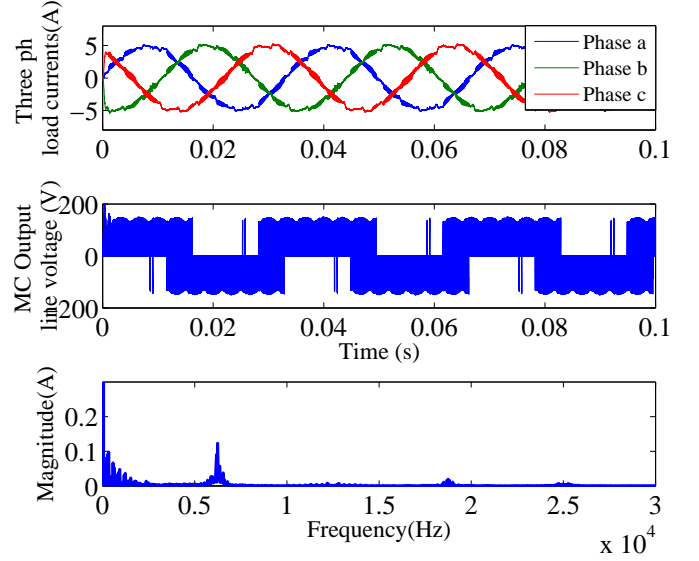


Fig. 6. Three phase load currents of MC controlled by M2PC

To demonstrate the fast dynamic response of M2PC, a step change from 2A to 4A and then to 2A. The resulting waveform is shown in Fig. 7 (top).
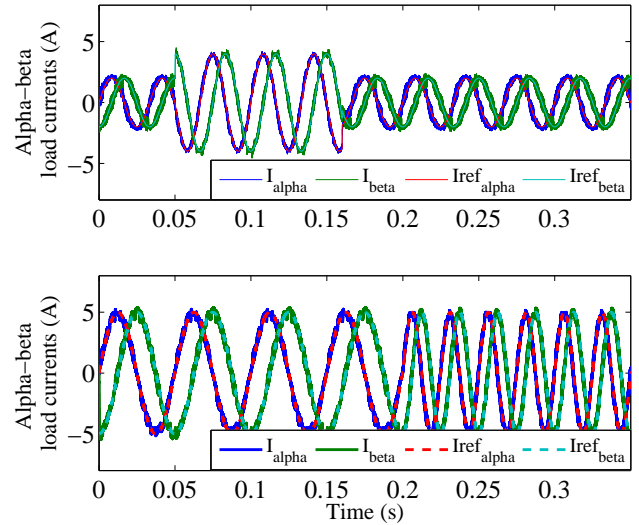


Fig. 7. Alpha-beta currents when the frequency of reference is changed

It is evident from the figure that the load current immediately follows the step demand in reference current and reaches steady state immediately. This indicates that M2PC can provide fast transient response which is a characteristic it inherited from MPC. In addition to the step change in current reference magnitude, a step change in the frequency of the current reference from 20Hz to 40Hz is also introduced.The resulting waveform is shown in Fig. 7 (bottom). The results indicate that M2PC is able to handle any abrupt changes in the reference signal without any overshoots or instability.

In order to conduct a quantitative analysis of the transient

response of the M2PC controller, load current control of matrix converter is implemented using MPC and a conventional PI Controller. The system parameters for the three methods remain constant. A step demand in load current amplitude from 2A to 4A is applied to the controller and the resulting d-axis load currents with the reference signal for all the three control methods is shown in Fig. 8. To conduct a fair analysis of the transient response of the controllers considered, the PI controller is tuned to achieve very fast response to set a benchmark for the comparison.

The simulation results for load current control of a direct MC with RL load are considered to compare the performance of M2PC controller with PI Controller and MPC. The THD of the currents controlled by the three methods can be considered as a measure of their steady state performance. To analyse the transient performance of the control strategies, the rise time of the controlled currents during a step change is considered. Rise time is the time taken by the control variable to reach from 10% to 90% of the steady state value. A comparison of the THDs and rise times for load current control of a MC for different controllers such as PI controller, MPC and M2PC from simulation results is tabulated in Table. II.
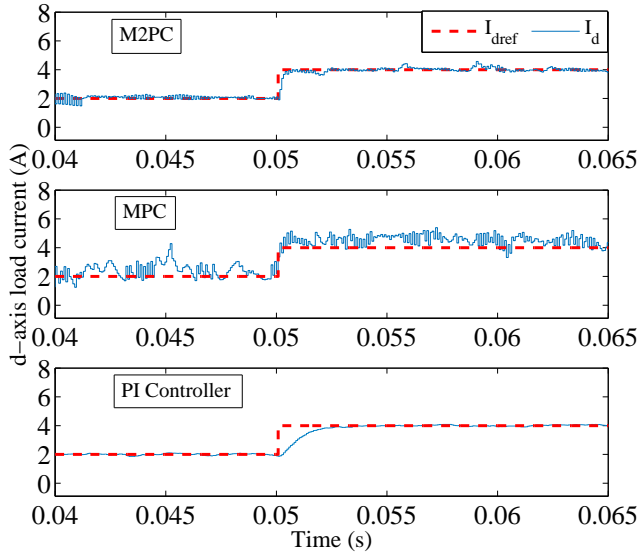


Fig. 8.  d-axis load current with reference during a step change in the amplitude

TABLE II
COMPARISON OF THDS AND RISE TIMES OF LOAD CURRENTS FOR DIFFERENT CONTROL STRATEGIES

| Control Strategy | Steady State Performance(THD) | Transient Performance (Risetime) |
|---|---|---|
| PI Controller | 1.89% | 4.1ms |
| MPC | 8.09% | 0.34ms |
| M2PC | 6.3% | 0.65ms |

From Table. II it can be seen that PI Controller with SVM

resulted in waveforms with least harmonic distortion followed by M2PC. MPC resulted in waveforms with the worst current quality. Predictive control based algorithms such as MPC and M2PC had faster dynamic response with rise times of 0.34ms and 0.65ms respectively; compared to that of PI controller that resulted in a rise time of 4.1ms. These results prove that M2PC is capable of fast dynamic response very similar to that of MPC when compared to a traditional PI controller and deliver waveforms with enhanced current quality compared to MPC.

## V. EXPERIMENTAL RESULTS

To validate the simulation results discussed in the previous section, the M2PC is implemented on a matrix converter feeding an RL load in the laboratory. The parameters of the system are given in Table. I.
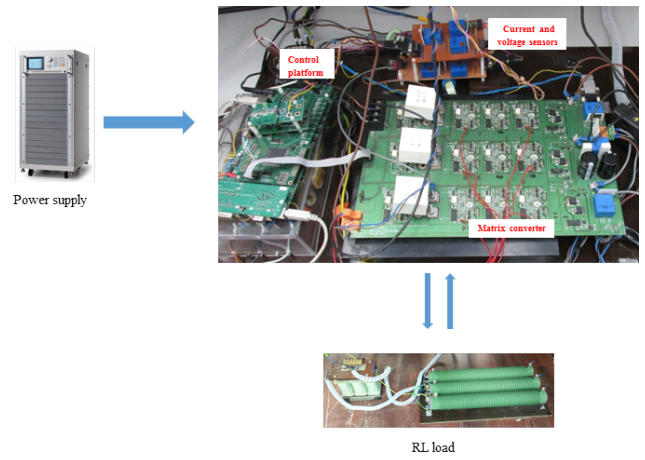


Fig. 9.  Experimental setup

The experimental setup shown in Fig. 9 includes a matrix converter using SK60GM123 IGBT modules rated at 1200V and 60A, a current direction detection circuit for four step commutation and a clamp circuit for over voltage protection. Each IGBT module consists of two diodes and two anti-parallel IGBT connected in the common emitter configuration. There are three current sensors to measure the output currents and three voltage sensors to measure the supply voltage to the converter. The control platform includes a Texas instrument DSP and a FPGA card developed at Power Electronics Machines and Control (PEMC) Group, The University Of Nottingham. The M2PC algorithm is implemented on the DSP at a sampling frequency of $80\mu$ s. An FPGA interface with the DSP ensures the four-step commutation of the switches. The setup is powered using Chroma Programmable AC source as indicated in Fig. 9.

The load currents of the direct matrix converter are controlled using the M2PC strategy. A reference current of 5A at 30Hz is demanded from the system and the experimental results of controlled load currents, MC output line voltage and the harmonic spectrum of Phase A load current are shown in Fig. 10. It is evident from Fig. 10 that the load currents are sinusoidal and reaches the steady state value without any error. The THD of the controlled waveforms is approximately

10.8%. The harmonic spectrum of Phase A load current reveals harmonics in the range of switching frequency (12.5kHz) and its multiples which confirms fixed switching frequency operation. This validates the simulation results shown in Fig. 6.
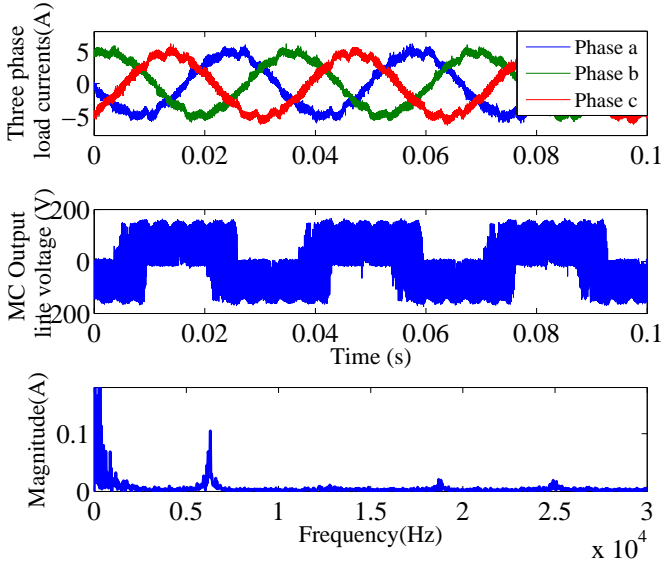


Fig. 10. Phase A load current, MC output line voltage and harmonic spectrum of load current at steady state

To analyse the transient behavior of the control strategy, a step demand in the amplitude and frequency of the reference current waveform is applied. A step in the amplitude of reference current waveform from 2A to 4A is applied and the frequency of the reference load current is changed from 20Hz to 40Hz and the resulting waveforms are shown in Fig. 11.
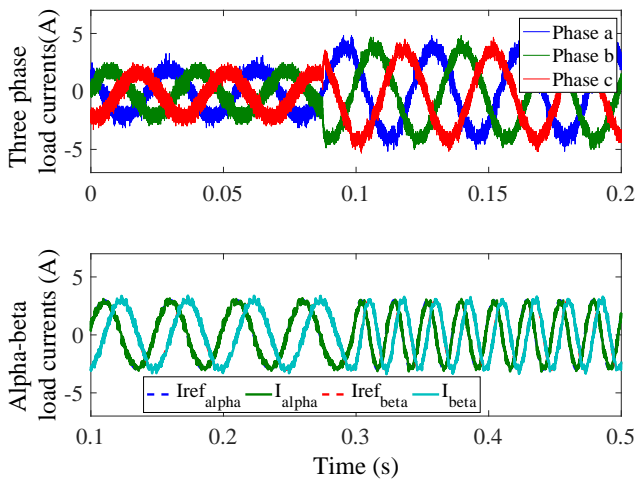


Fig. 11. Dynamic performance of M2PC during step change in the magnitude(top) and frequency(bottom) of the reference load current

From Fig. 11, it is evident that the load currents respond to the sudden changes in amplitude and frequency instantaneously without any delay. The results from the experimental tests conforms to the simulation results which proves the system model and control strategy. To summarize, the load current control achieved by this method is characterized by very fast transient response as in the case of MPC and an improved steady state response due to the presence of an inbuilt modulation scheme.

## VI. Effect of Sampling Time on Waveform Quality

Since the performance of MPC is largely dependant on the sampling interval, it is worth studying if this applies to the M2PC. For MPC, quality of the controlled currents are improved as the sampling interval gets smaller. To analyse the effect of sampling time on the quality of the controlled waveforms in this case the load currents, the M2PC strategy is implemented for three different sampling times such as $50\mu s, 80\mu s$ and $100\mu s$. The quality of the controlled currents are assessed by comparing the THDs for these sampling times. Both simulation and experimental tests are conducted for three different sampling intervals or switching frequencies and the THDs of the resulting current waveforms are tabulated as shown in Table. III.

TABLE III
COMPARISON OF THDS FOR M2PC WITH DIFFERENT SAMPLING INTERVALS

| Sampling time | Total Harmonic Distortion | |
| --- | --- | --- |
| | *Simulation Results* | *Experimental Results* |
| $50\mu s$ | 4.0% | 7.33% |
| $80\mu s$ | 6.3% | 10.8% |
| $100\mu s$ | 7.5% | 12.07% |

Table. III indicates that there is a considerable effect on the quality of the controlled waveforms as the sampling interval is changed. The current quality was the best when a sampling time of $50\mu s$ is considered and the worst when the sampling time is $100\mu s$. It is interesting to note that the M2PC strategy is also dependant on the sampling interval considered which is expected as it is predominantly a predictive control based method.

## VII. Conclusion

A control method with the features of MPC and a modulation scheme similar to SVM is proposed in this paper for a direct matrix converter drives. The ability to control different parameters simultaneously, high controller bandwidth and constant switching frequency are the main highlights of this method. The constant switching behavior of the SVM utilised in this method guarantees that a predictive based control method can now be used where the traditional associated problems with input filter sizing, harmonic performance, switching loss and hence thermal management design can now be addressed in a more predictable and systematic way. A comparison of the performance of M2PC with control methods such as MPC and PI controller showed that M2PC is capable of fast dynamic response. The experimental results presented in this paper validates the M2PC strategy for load current control of a direct matrix converter.

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